

New Design of Miniature C-Band Substrate Integrated Waveguide Bandpass Filters Using Ceramic Material

Ahmed Rhbanou

Group MIN, ESTM
Superior School of Technology
Moulay Ismail University - Meknes
Morocco

Adiba EL Fadl

High Energy Physics - Modeling and
Simulation. (LPHE-MS)- Sciences Faculty,
Mohamed 5 University - Rabat
Morocco

Nawfal Jebbor

Full Professor
Group MIN, ESTM
Superior School of Technology
Moulay Ismail University - Meknes
Morocco

Seddik Bri

Full Professor
Group MIN, ESTM
Superior School of Technology
Moulay Ismail University - Meknes
Morocco

This article presents new structures and methods of design of miniature third-order substrate integrated waveguide (SIW) bandpass filters on a high-permittivity ceramic substrate for the C-band. The aim was to appraise the feasibility of such filters by using a 3D electromagnetic (EM) simulator. The substrate integrated waveguide (SIW) offers good quality factors and electrical performances compared with other planar techniques. Its integration capabilities and fabrication cost are other benefits that make it attractive. Ceramic material offer electrical properties suitable in designing of passive devices. High relative permittivity with low dielectric losses makes it possible to miniaturize passive components while exhibiting high temperature stability, which is an important selection criterion for a filter designed to equip the payload of a satellite. Three SIW filters were designed on a Trans-Tech ceramic substrate (thickness = 254 μm , $\epsilon_r = 90$, and $\tan\delta = 0.0009$) with drastic specifications for space application. The first filter is composed of three SIW resonators with direct coupling, the second is composed of three SIW resonators with a cross-coupling to create a transmission zero, and the third is composed of three SIW resonators with circular holes etched on the top of the metal layer to achieve a super-wide band. The obtained results for the proposed filters are presented, discussed, and compared with relevant published literature. The proposed filter can be used to enhance the performance of microwave devices used for C-band, especially Satellite communications.

Keywords: Ceramic material, Cross-coupling, High-Permittivity, Substrate integrated waveguide (SIW), Bandpass filter

1. INTRODUCTION

Ceramic materials offer relevant dielectric characteristics for the conception of passive devices [1,2]. Some of them reach high relative permittivity while presenting low dielectric losses ($\tan\delta < 0.001$) [3-5]. They show themselves also very stable against temperature changes, an essential criterion for a filter used in spatial applications [6]. However, the realization of miniature filters is confronted by more restrictive technological constraints (a narrower microstrip line and finer drillings).

A substrate integrated waveguide (SIW) allows integration of the rectangular waveguide into a substrate through two arrays of via holes [7,8]. These vias must all have the same diameter and must have sufficiently small spacing to appear as perfect electric walls [9-11]. A recent work on the state-of-the-art of the SIW technology makes an inventory of the main published papers on SIW filters [12-24]. Most of the SIW filters were designed on a standard alumina substrate with excellent

performances of low insert loss and high Q factor compared with the other planar techniques. However, the dimensions of these SIW filters are so large that they are difficult to integrate in satellite payload equipment.

In this paper, we propose to design SIW filters on a high-permittivity ceramic substrate for the C-band in order to achieve drastic specifications for space application with the best compromise between size and electrical performances. We begin with the design of a third-order direct-coupled SIW filter on a standard alumina substrate (thickness = 254 μm , $\epsilon_r = 9.9$, and $\tan\delta = 0.0003$) and then conceive its equivalent (the same order, the same frequencies) on a Trans-Tech ceramic substrate (thickness = 254 μm , $\epsilon_r = 90$, and $\tan\delta = 0.0009$).

The results obtained are compared in order to evaluate the performance of the high-permittivity ceramic. Then, two other third-order SIW filters are designed on a substrate with a relative permittivity of 90, the first one with a cross-coupling between resonators to create a transmission zero and the second with circular holes etched on the top of the metal layer to achieve a super-wide bandpass. Gold metal walls ($\sigma = 41 \times 10^6 \text{ S/m}$) with a thickness of 4 μm will be used for the metallization. The structures will be simulated by using the available Ansoft software High Frequency Structure Simulator (HFSS).

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Correspondence to: Seddik Bri, Group Material and
Instrumentations MIN, Superior School of Technology,
Moulay Ismail University Meknes, Morocco
E-mail: seddikbri@gmail.com

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2. DESIGN OF THE C-BAND THIRD-ORDER DIRECT-COUPLED SIW BANDPASS FILTER

The filter must exhibit electrical specifications of a central frequency of 5.24 GHz with an 8% fractional bandwidth. The return loss must be better than 20 dB in the whole passband and the attenuation must be higher than 20 dB for frequencies ≥ 5.7 GHz. The coupling structure of this filter is shown in Fig. 1.

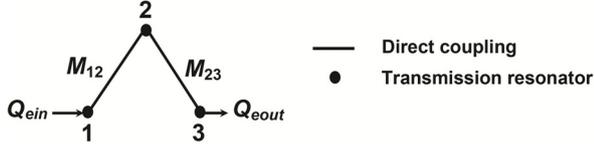


Figure 1. Coupling structure of the third-order direct-coupled SIW bandpass filter.

where Q_{ein} and Q_{eout} are the external quality factors of the resonators at the input and at the output, and M_{12} and M_{23} are the coupling coefficients between the resonators. The external quality factors (Q_{ein} , Q_{eout}) and the coupling matrix $[m]$ of this filter are given by (1) and (2), respectively.

$$Q_{\text{ein}} = Q_{\text{eout}} = 10.6682 \quad (1)$$

$$[m] = \begin{bmatrix} 0 & 1.03027 & 0 \\ 1.03027 & 0 & 1.03027 \\ 0 & 1.03027 & 0 \end{bmatrix} \quad (2)$$

where m_{ij} denotes the so-called normalized coupling coefficient [25].

$$m_{ij} = \frac{M_{ij}}{FBW} \quad \text{for } i, j = 1, 2, \dots, n \quad (3)$$

where n is the order of the filter and FBW is the designed fractional bandwidth.

2.1 SIW filter designed on a substrate ($\epsilon_r=9.9$)

The substrate used is alumina with a permittivity of 9.9, a thickness of 254 μm , and $\tan\delta = 0.0003$. A 50- Ω microstrip line designed on this substrate at a frequency of 5.24 GHz corresponds to a width of $W_M = 0.24$ mm and therefore this access line can be realized. The impedance matching between the SIW filter and the 50- Ω lines is made by intermediate transitions between them [26-28]. The physical dimensions of these transitions control the external quality factors of the filter.

The external quality factor Q_e can be extracted from the structure shown in Fig. 2, an SIW square cavity (P , D , and $W_{\text{SIW1}} = L_{\text{SIW1}}$) coupled to a 50- Ω access line (W_M and L_M) via a microstrip transition (W_T and L_T). This structure must be well sized to have a resonance frequency of 5.24 GHz (TE_{101} mode). The dimensions are obtained by applying the equations and rules adopted in [29-33], namely $D = 0.2$ mm, $P = 0.5$ mm, $W_{\text{SIW1}} = L_{\text{SIW1}} = 11.8$ mm, $W_T = 4.72$ mm, $W_M = 0.24$ mm, and $L_M = 1.2$ mm. The parameter involved in the study of this coupling is the length L_T of the tapered-microstrip transition. The value of Q_e is obtained from the simulation and the use of the following equation [34, 35]:

$$Q_e = \frac{f_0}{\Delta f_{\pm 90^\circ}} \quad (4)$$

where f_0 is the resonant frequency of the SIW cavity and $\Delta f_{\pm 90^\circ}$ is the $\pm 90^\circ$ bandwidth of the SIW cavity. Fig. 3 shows the variation of Q_e as a function of L_T .

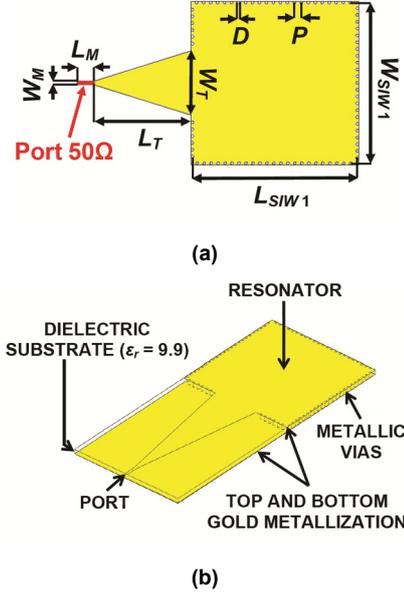


Figure 2. Arrangement for extracting the external quality factor Q_e . (a) Top view. (b) Three-dimensional (3D).

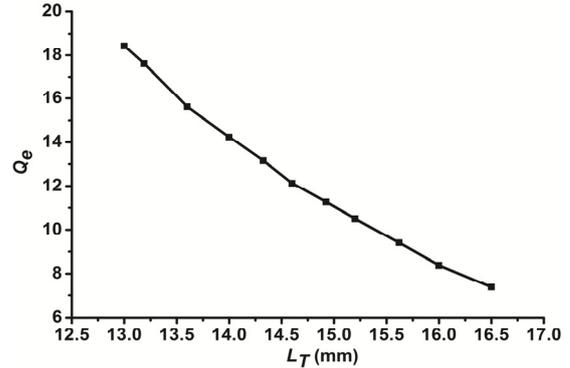


Figure 3. External coupling Q_e as a function of parameter L_T .

We can see that the external quality factor Q_e decreases when the length L_T of the tapered-microstrip transition becomes larger and larger. Thus, as required for filter specifications, $Q_{\text{ein}} = Q_{\text{eout}} = 10.6682$ is obtained when $L_T = 15.1$ mm. The coupling coefficient M_{12} can be extracted from the structure shown in Fig. 4. An SIW square cavity with a resonance at 5.75 GHz coupled to another SIW cavity with a resonance at 5.47 GHz via an iris opening d_{12} . M_{12} is obtained from the simulation by [36,37]:

$$M = \pm \frac{1}{2} \left(\frac{f_{02}}{f_{01}} + \frac{f_{01}}{f_{02}} \right) \sqrt{\left(\frac{f_2^2 - f_1^2}{f_2^2 + f_1^2} \right)^2 - \left(\frac{f_{02}^2 - f_{01}^2}{f_{02}^2 + f_{01}^2} \right)^2} \quad (5)$$

where f_{01} and f_{02} are the self-resonant frequencies of the first and second resonators, respectively, and f_1 and f_2 represent the lower and higher resonant frequencies, respectively, obtained from the EM-simulated results. Fig. 5 shows the evolution of the coupling coefficient

M_{12} as a function of the iris opening d_{12} . We can see that the increase of the iris opening produces an increase of the coupling coefficient. Thus, as required for the filter specifications, $M_{12} = M_{23} = 0.08242$ is obtained for an iris opening equal to 7.4 mm.

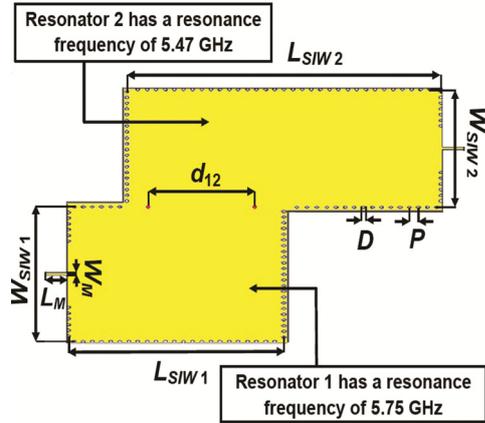


Fig. 4. Top view of arrangement for extracting coupling coefficient M_{12} , where $D = 0.2$ mm, $P = 0.5$ mm, $W_{SIW1} = L_{SIW1} = 11.8$ mm, $W_{SIW2} = 10.2$ mm, $L_{SIW2} = 17.2$ mm, $W_M = 0.24$ mm, and $L_M = 1.2$ mm.

The geometrical structure of the third-order direct-coupled SIW band pass filter on an alumina substrate ($\epsilon_r = 9.9$) is shown in Fig. 6. The dimensions of this filter are optimized by the HFSS software in order to obtain the desired frequency response (Table 1).

From the simulation results (Fig. 7 (a)), the filter has a 3-dB bandwidth of 0.41 GHz (a fractional bandwidth of 7.8%) and an insertion loss of 2.43 dB at a centre frequency of 5.24 GHz. It also has a return loss better than 18.5 dB from 5.02 to 5.28 GHz and a rejection level higher than 20 dB from 6.05 to 6.67 GHz. We also note that the group delay of S_{21} , shown in Fig. 7 (b), is 1.98 ns at 5.24 GHz with a variation of 1.1 ns in the passband (from 4.98 to 5.39 GHz). Note that the surface area of the filter is 53.4 mm \times 22.2 mm = 1185.5 mm² (Fig. 6).

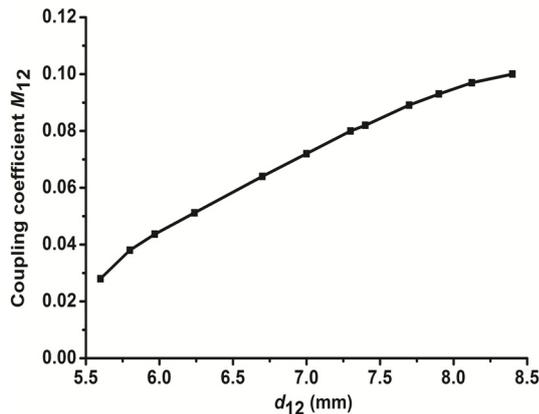


Figure 5. Coupling coefficient M_{12} versus parameter d_{12} .

Table 1: Dimensions of the third-order direct-coupled siw bandpass filter on a standard alumina substrate

Symbol	Value (mm)	Symbol	Value (mm)	Symbol	Value (mm)
D	0.2	W_{SIW2}	10.2	W_T	4.72
P	0.5	L_{SIW2}	17.2	L_T	13.6
W_{SIW1}	11.8	W_M	0.24	d_{12}	5.6
L_{SIW1}	11.8	L_M	1.2	d_{23}	5.6

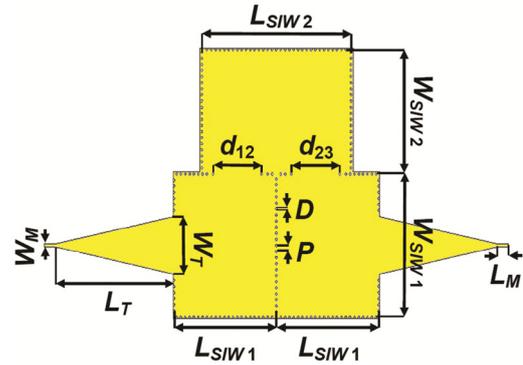


Figure 6. Top view of the third-order direct-coupled SIW bandpass filter on a standard alumina substrate ($\epsilon_r=9.9$).

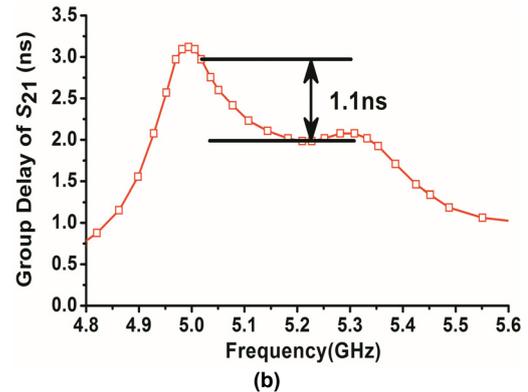
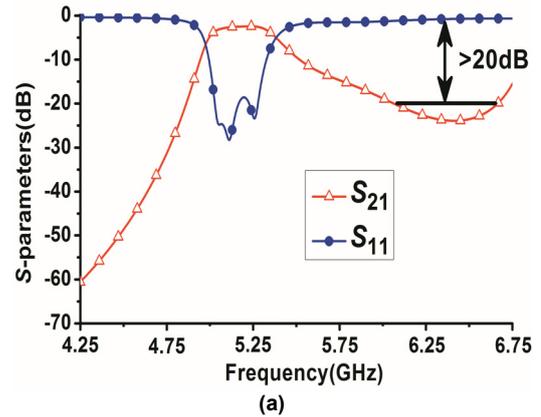


Figure 7. Simulated results of the third-order direct-coupled SIW bandpass filter on a standard alumina substrate ($\epsilon_r=9.9$). (a) S-parameters. (b) Group delay of S_{21} .

2.2 SIW filter designed on a high-permittivity substrate ($\epsilon_r=90$)

The third-order direct-coupled SIW bandpass filter on a high-permittivity ceramic substrate is designed by following the same process of design as for a third-order direct-coupled SIW bandpass filter on a standard alumina substrate ($\epsilon_r = 9.9$). The selected substrate was provided by Trans-Tech. Its relative permittivity is 90, thickness is 254 μ m, and the loss tangent is less than 0.0009. The access line that we used on this substrate has a width of $W_M=0.17$ mm, which corresponds to a characteristic impedance of 20 Ω at 5.24 GHz. As a result, the 50- Ω lines are eliminated due to the fineness of the corresponding line width (of the order of 5.8 μ m). Then, using equation (4) and the same structure as in Fig. 2 under the conditions of $D = 0.2$ mm, $P = 0.5$ mm, $W_{SIW1} = L_{SIW1} = 4$ mm, $W_T = 1$ mm, $W_M = 0.17$ mm, and $L_M = 1$

mm, we are able to present the variation of Q_e as a function of L_T (Fig. 8). We can thus see that the external quality factor Q_e obtained by the synthesis, whose value is 10.6682, implies the use of a length of $L_T = 1.15$ mm.

In the same way, for the coupling between the adjacent cavities ($M_{12} = M_{23}$), using equation (5) and the structure of Fig. 4 under the conditions of $D = 0.2$ mm, $P = 0.5$ mm, $W_{SIW1} = L_{SIW1} = 4$ mm, $W_{SIW2} = 3.305$ mm, $L_{SIW2} = 6$ mm, $W_M = 0.17$ mm, and $L_M = 1$ mm, we obtain the variation of the coupling coefficient M_{12} as a function of the iris opening d_{12} (Fig. 9). We can thus observe that $M_{12} = M_{23} = 0.08242$ is obtained for an iris opening equal to 2.68 mm.

The configuration and optimal physical dimensions of the third-order direct-coupled SIW bandpass filter on a high-permittivity ceramic substrate ($\epsilon_r = 90$) are shown in Fig. 10 and Table 2, respectively. We note that the surface area is $12.4 \text{ mm} \times 7.675 \text{ mm} = 95.17 \text{ mm}^2$, which represents a considerable miniaturization with a nearly 92% reduction in the surface area compared to the filter on an alumina substrate (Fig. 6). The results obtained with HFSS (Fig. 11) proved that the fractional bandwidth is 8% and the insertion loss is 2.66 dB at the centre frequency of 5.24 GHz. Thus, the return loss is better than 20 dB from 5.09 to 5.35 GHz, the rejection level is higher than 20 dB from 5.7 to 6.6 GHz, and the variation of group delay is less than 0.61 ns in the passband.

These results confirm that the proposed filter on a substrate with a relative permittivity of 90 (Fig. 10) satisfies the required specifications with a very significant size reduction.

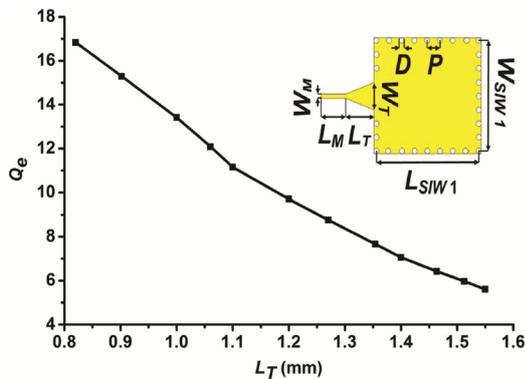


Figure 8. Q_e as a function of L_T , where $D = 0.2$ mm, $P = 0.5$ mm, $W_{SIW1} = L_{SIW1} = 4$ mm, $W_T = 1$ mm, $W_M = 0.17$ mm, and $L_M = 1$ mm.

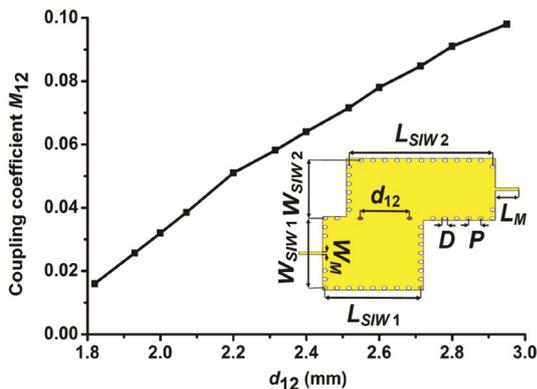


Figure 9. M_{12} as a function of d_{12} , where $D = 0.2$ mm, $P = 0.5$ mm, $W_{SIW1} = L_{SIW1} = 4$ mm, $W_{SIW2} = 3.305$ mm, $L_{SIW2} = 6$ mm, $W_M = 0.17$ mm, and $L_M = 1$ mm.

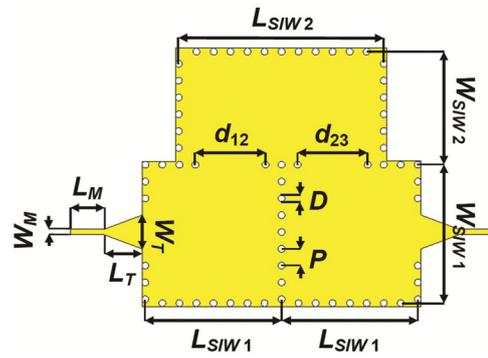


Fig. 10. Top view of the third-order direct-coupled SIW bandpass filter on a high-permittivity ceramic substrate ($\epsilon_r = 90$).

Table 2: Dimensions of the third-order direct-coupled SIW bandpass filter on a high-permittivity ceramic

Symbol	Value (mm)	Symbol	Value (mm)	Symbol	Value (mm)
D	0.2	W_{SIW2}	3.36	W_T	1
P	0.5	L_{SIW2}	6	L_T	1.1
W_{SIW1}	4.115	W_M	0.17	d_{12}	2.06
L_{SIW1}	4	L_M	1	d_{23}	2.06

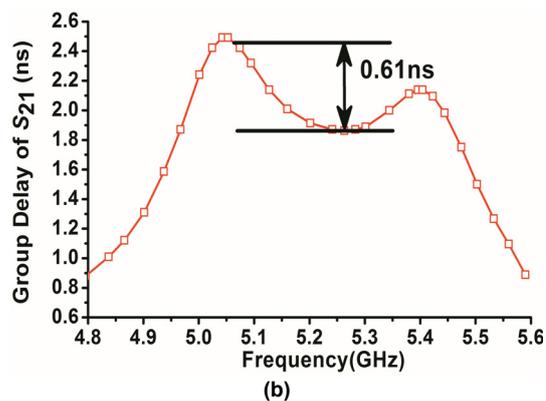
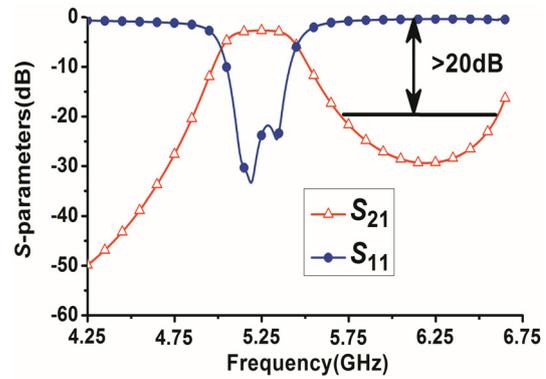


Fig. 11. Simulated results of the third-order direct-coupled SIW bandpass filter on a high-permittivity ceramic substrate ($\epsilon_r=90$). (a) S-parameters. (b) Group delay of S_{21} .

3. DESIGN C-BAND THIRD-ORDER CROSS-COUPLED SIW BANDPASS FILTER WITH CERAMIC SUBSTRATE

This filter must be centered at 5.24 GHz with a fractional bandwidth of 8% and a rejection of 52 dB at 5.77 GHz. The substrate used is also the ceramic substrate with a relative permittivity of 90, a thickness of $254 \mu\text{m}$, and $\tan\delta = 0.0009$. The coupling structure of this filter is shown in Fig. 12.

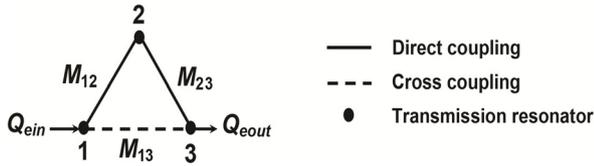


Fig. 12. Coupling structure of the third-order SIW bandpass filter with cross-coupling between resonators 1 and 3.

The normalized coupling matrix $[m]$ and the external quality factors (Q_{ein} , Q_{eout}) of this filter are given as follows:

$$[m] = \begin{bmatrix} 0.075 & 0.99777 & 0.29859 \\ 0.99777 & -0.29067 & 0.99777 \\ 0.29859 & 0.99777 & 0.075 \end{bmatrix} \quad (6)$$

$$Q_{ein} = Q_{eout} = 10.6671 \quad (7)$$

Then, by following the same method of design as for the third-order direct-coupled SIW bandpass filter on a high-permittivity ceramic substrate (Fig. 10), we can obtain the results presented in Figs. 8 and 9. From these results, we can extract the dimensions of the coupling elements (L_T , d_{12} , and d_{23}). Table 3 presents the coupling coefficients to be applied with their correspondence in the physical dimension.

Table 3. Coupling coefficients to be applied with their correspondence in the physical dimension

Coupling Coefficients	Dimensions of Coupling Elements (mm)
$Q_e = 10.6671$	$L_T = 1.15$
$M_{12} = M_{23} = 0.07982$	$d_{12} = d_{23} = 2.62$

The cross-coupling between resonators 1 and 3 is achieved by an iris d_{13} (Fig. 13). The cross-coupling coefficient M_{13} is obtained from the simulation by [38]-[40]:

$$M = \pm \frac{f_2^2 - f_1^2}{f_2^2 + f_1^2} \quad (8)$$

where f_1 and f_2 also represent the lower and higher resonant frequencies, respectively, obtained from the EM-simulated results. Fig. 14 shows the evolution of the cross-coupling coefficient M_{13} as a function of the iris opening d_{13} , where $D = 0.2$ mm, $P = 0.5$ mm, $W_{SIW1} = L_{SIW1} = 4$ mm, $W_M = 0.17$ mm, and $L_M = 1$ mm. From this abacus, we can see that the cross-coupling coefficient $M_{13} = 0.02388$ is obtained for an iris opening equal to 1.5 mm.

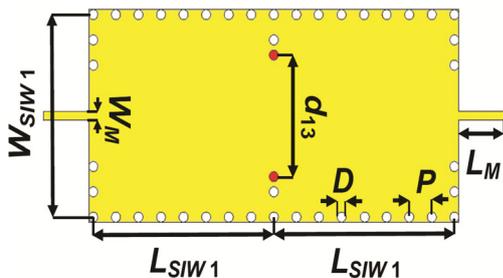


Fig. 13. Top view of arrangement for extracting the cross-coupling coefficient M_{13} .

The geometrical structure and optimal dimensions of the third-order cross-coupled SIW bandpass filter on a

high-permittivity ceramic substrate ($\epsilon_r = 90$) are shown in Fig. 15 and Table 4, respectively. Based on the simulated frequency response in HFSS (Fig. 16), the filter has a fractional bandwidth (FBW) of 8% and an insertion loss (IL) of 2.57 dB at a centre frequency (CF) of 5.24 GHz. It also has a return loss better than 20 dB from 5.12 to 5.4 GHz and attenuation of 51.65 dB at 5.77 GHz.

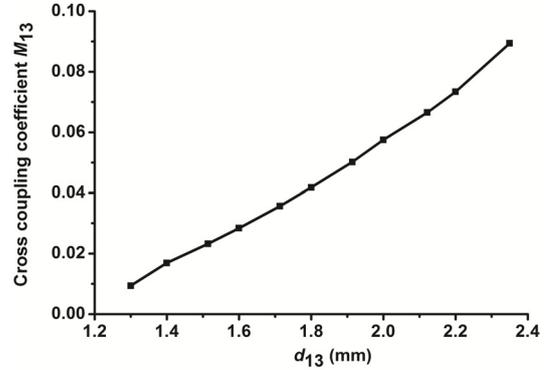


Fig. 14. Cross-coupling coefficient M_{13} versus parameter d_{13} , where $D = 0.2$ mm, $P = 0.5$ mm, $W_{SIW1} = L_{SIW1} = 4$ mm, $W_M = 0.17$ mm, and $L_M = 1$ mm.

In order to examine the precision of the obtained results, we compared them with published results in [41]. Table 5 illustrates the comparison between the third-order cross-coupled SIW bandpass filter on a high-permittivity ceramic substrate ($\epsilon_r = 90$) and the filters presented in [41]. From this comparison, we have demonstrated that the proposed filter (Fig. 15) has low insertion loss, a good upper stopband (30 dB from 5.6 to 6.6 GHz), and a very compact size compared to the SIW filters presented in [41], which are designed on the same high-K substrate ($\epsilon_r = 90$). We conclude that the proposed filter (Fig. 15) has the advantage of compact size that is easy to integrate with other planar circuits and good out-band suppression with simple structure.

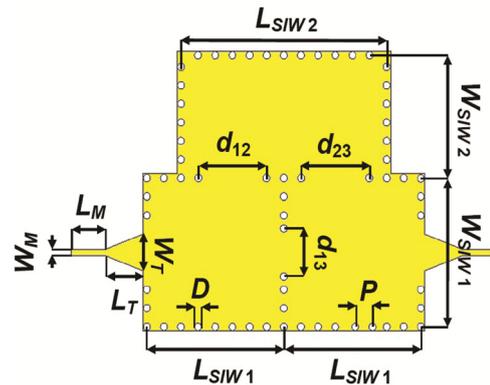


Fig. 15. Top view of the third-order cross-coupled SIW bandpass filter on a high-permittivity ceramic substrate ($\epsilon_r = 90$).

Table 4. Dimensions of the third-order cross-coupled SIW bandpass filter on ceramic substrate

Symbol	Value (mm)	Symbol	Value (mm)	Symbol	Value (mm)
D	0.2	L_{SIW2}	6	L_T	1.1
P	0.5	W_M	0.17	d_{12}	1.98
$W_{SIW1} = L_{SIW1}$	4	L_M	1	d_{23}	1.98
W_{SIW2}	3.305	W_T	1	d_{13}	1.3

Table 5: Results comparison with the presented filters in [41]

Ref.	Technology	Order	CF (GHz)	FBW (%)	IL (dB)	Upper-Band Rejection	Size (mm ³)
[41]	High-K Ceramic ($\epsilon_r=90$)/SIW	6	4	7.2	2.6	30dB 4.25-5 GHz	26.34×14.24×0.635
[41]	High-K Ceramic ($\epsilon_r=90$)/SIW	8	4	8	2.95	30dB 4.25-5 GHz	33.12×14.64×0.635
This work (Fig. 15)	High-K Ceramic ($\epsilon_r=90$)/SIW	3	5.24	8	2.57	30dB 5.6-6.6 GHz	12.4×7.505×0.254

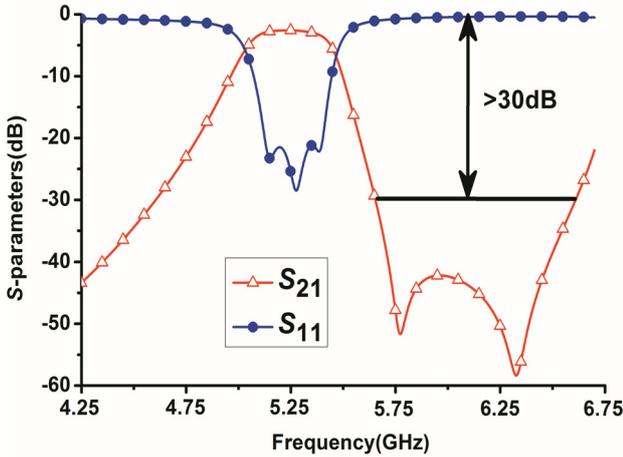
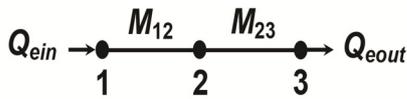


Fig. 16. Simulated frequency response of the third-order cross-coupled SIW bandpass filter on a high-permittivity ceramic substrate ($\epsilon_r = 90$).

4. DESIGN C-BAND THIRD-ORDER DIRECT-COUPLED SUPER-WIDE BANDPASS SIW FILTER WITH A CERAMIC SUBSTRATE

This filter must exhibit performances of a centre frequency of 6.9 GHz with a ripple of 0.1 dB and a fractional bandwidth of 38%. The substrate used is also a ceramic substrate with a relative permittivity of 90, a thickness of 254 μm , and a loss tangent of 0.0009. The coupling structure (Fig. 17), the normalized coupling matrix $[m]$, and the external quality factors (Q_{ein} , Q_{eout}) of this filter are given below:



— Direct coupling ● Transmission resonator

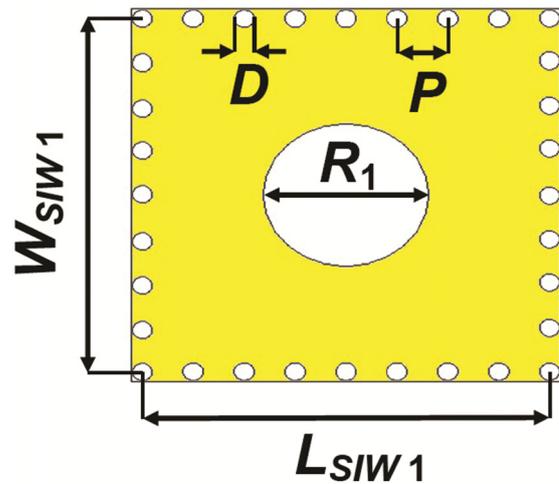
Fig. 17. Coupling structure of the third-order direct-coupled super-wide bandpass SIW filter.

$$[m] = \begin{bmatrix} 0 & 0.9071 & 0 \\ 0.9071 & 0 & 0.9071 \\ 0 & 0.9071 & 0 \end{bmatrix} \quad (9)$$

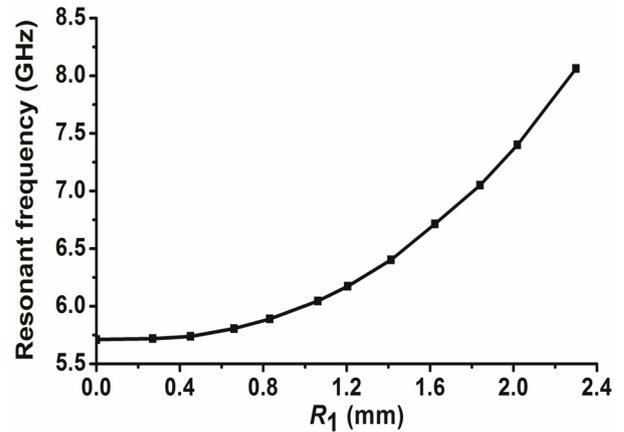
$$Q_{\text{ein}} = Q_{\text{eout}} = 2.7806 \quad (10)$$

Fig. 18 (a) shows the structure of the SIW cavity with a circular hole etched on the top of the metal layer. The dimensions of the SIW cavity are fixed ($P = 0.2$ mm, $D = 0.5$ mm, and $W_{\text{SIW}1} = L_{\text{SIW}1} = 4$ mm) and therefore the resonant frequency depends only on the diameter R_1 of the circular hole. Fig. 18 (b) shows the variation of the resonant frequency as a function of R_1 .

We notice that an increase in the diameter R_1 of the circular hole makes it possible to shift the resonant frequency towards a higher frequency. We can therefore reach the desired frequency (6.9 GHz) by applying a diameter of $R_1 = 1.624$ mm.



(a)



(b)

Fig. 18. (a) Top view of the SIW cavity with a circular hole etched on the top of the metal layer, where $D = 0.2$ mm, $P = 0.5$ mm, and $W_{\text{SIW}1} = L_{\text{SIW}1} = 4$ mm. (b) Resonant frequency as a function of parameter R_1 .

Then, using a Conductor Backed Coplanar Waveguide (CBCPW) as a transition to connect a microstrip line to an SIW square cavity with a circular hole etched on the top of the metal layer (Fig. 19 (a)), we can extract the external quality factor Q_e . The parameter involved in the study of Q_e is the length L_{CPW} of CBCPW transition. Fig. 19 (b) shows the variation of Q_e as a function of L_{CPW} , where $D = 0.2$ mm, $P = 0.5$ mm, $W_{\text{SIW}1} = L_{\text{SIW}1} = 4$ mm, $R_1 = 1.624$ mm, $W_M = 0.28$ mm, $L_M = 0.88$ mm, and $W_{\text{CPW}} = 0.08$ mm.

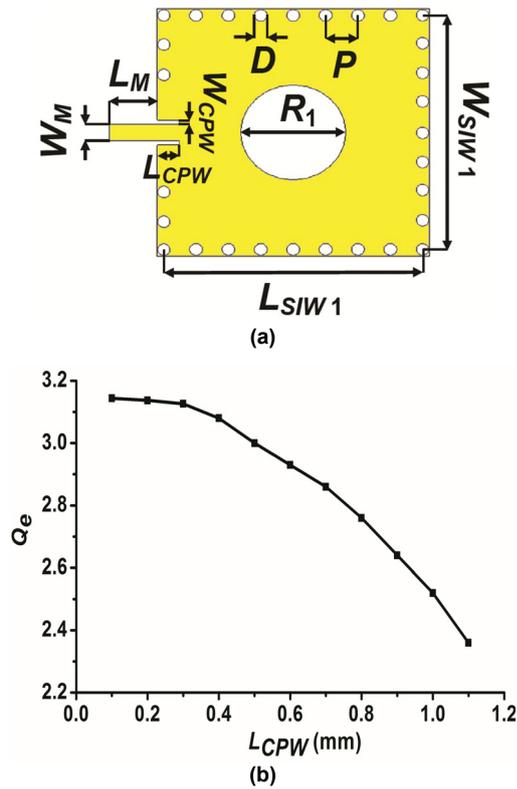


Fig. 19. (a) Top view of arrangement for extracting Q_e , where $D = 0.2$ mm, $P = 0.5$ mm, $W_{SIW1} = L_{SIW1} = 4$ mm, $R_1 = 1.624$ mm, $W_M = 0.28$ mm, $L_M = 0.88$ mm, and $W_{CPW} = 0.08$ mm. (b) Q_e as a function of L_{CPW} .

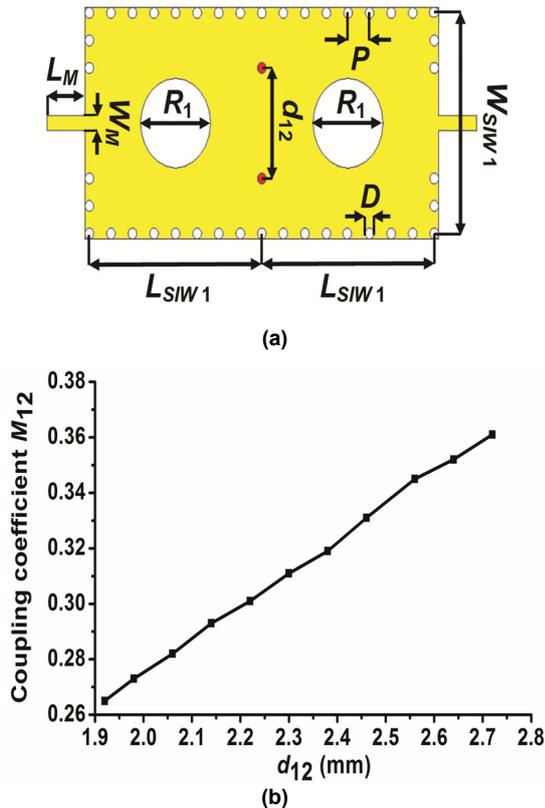


Fig. 20. (a) Top view of arrangement for extracting M_{12} , where $D = 0.2$ mm, $P = 0.5$ mm, $W_{SIW1} = L_{SIW1} = 4$ mm, $R_1 = 1.624$ mm, $W_M = 0.28$ mm, and $L_M = 0.88$ mm. (b) M_{12} as a function of d_{12} .

For the calculation of M_{12} , we simulate the structure of Fig. 20 (a): two resonators coupled by an iris opening. Each resonator consists of an SIW square cavity

with a circular hole etched on the top of the metal layer. Then, using equation (8) for each variation of the iris opening d_{12} with the conditions $D = 0.2$ mm, $P = 0.5$ mm, $W_{SIW1} = L_{SIW1} = 4$ mm, $R_1 = 1.624$ mm, $W_M = 0.28$ mm, and $L_M = 0.88$ mm, we can present the evolution of M_{12} as a function of d_{12} (Fig. 20 (b)).

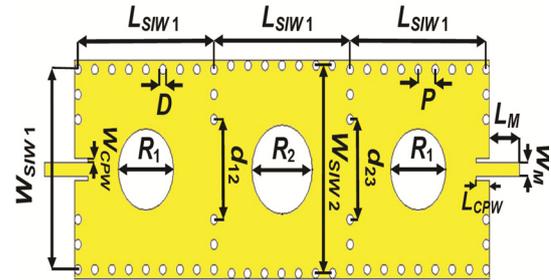


Fig. 21. Top view of the third-order direct-coupled super-wide bandpass SIW filter with a high-permittivity ceramic substrate ($\epsilon_r = 90$) and circular holes etched on the top of the metal layer.

The results presented in Fig. 19 (b) and Fig. 20 (b) make it possible to deduce the initial dimensions to be applied for the coupling elements (L_{CPW} and $d_{12} = d_{23}$). The configuration and the dimensions of the filter, after optimization by HFSS, are shown in Fig. 21 and Table 6, respectively.

The simulated frequency response by HFSS (Fig. 22) shows that the fractional bandwidth (FBW) is 38% at the centre frequency (CF) of 6.9 GHz and the return loss is better than 16 dB from 5.72 to 8.22 GHz. Thus, the minimum insertion loss (IL) is 1.26 dB and the ripple in the pass band is less than 0.18 dB. Compared with the filters using high-K ceramic [42], [43] as list in Table 7, it can clearly be seen that the proposed filter (Fig. 21) has better performances, including very low ripple, lower insertion loss and greater fractional bandwidth. Also, the proposed design gets a more compact circuit size than other designs.

Table 6: Dimensions of the proposed filter (Fig. 21)

Symbol	Value (mm)	Symbol	Value (mm)	Symbol	Value (mm)
D	0.2	W_{CPW}	0.08	d_{12}	2
P	0.5	L_{CPW}	0.4	d_{23}	2
$W_{SIW1} = L_{SIW1}$	4	W_M	0.28	R_1	1.624
W_{SIW2}	4.16	L_M	0.88	R_2	1.78

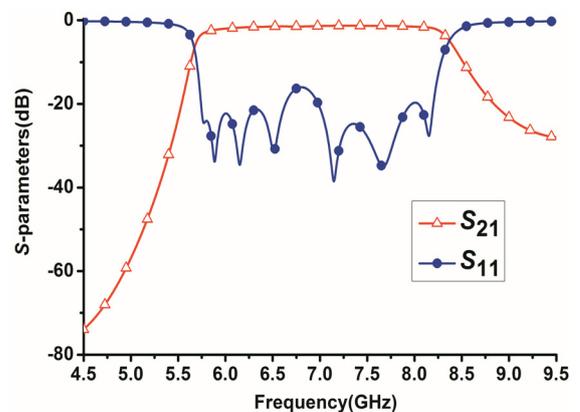


Fig. 22. Frequency response of the third-order direct-coupled super-wide band pass SIW filter with a high-permittivity ceramic substrate ($\epsilon_r = 90$) and circular holes etched on the top of the metal layer.

Table 7: Comparison with the published filters

Ref.	Technology	Order	CF (GHz)	FBW (%)	IL (dB)	Ripple (dB)	Surface (mm ²)
[42]	High-K Ceramic ($\epsilon_r=68.7$)/LTCC/SIW	6	7.33	5	3.9	2.1	16.375×4.3
[43]	High-K Ceramic ($\epsilon_r=90$)/Microstrip	5	3.83	23	1.12	1.27	13.51×6.75
This work (Fig. 21)	High-K Ceramic ($\epsilon_r=90$)/SIW	3	6.9	38	1.26	0.18	13.96×4.36

5. CONCLUSION

New miniature third-order SIW bandpass filters on a high-permittivity ceramic substrate for the C-band are presented in this article. The use of a ceramic substrate with a relative permittivity of 90 allowed us to reduce the surface area of the SIW filter by nearly 92% compared to the SIW filter on alumina substrate ($\epsilon_r = 9.9$). The simulation results also demonstrate that this reduction in size does not influence the performances of the filter, that is to say without strong degradation of the insertion losses, and from here we conclude that such particularly high-permittivity ceramics are very attractive for frequency applications between UHF and C-band. We have also proved that the use of a cross-coupling between the resonators allows improvement of the rejection. Then, we have proposed a novel miniature C-band super-wide bandpass SIW filter by using a high-permittivity ceramic substrate and circular holes etched on the top of the metal layer. The simulation results of the proposed filters are encouraging and filled the design criteria for radio frequency (RF) such as low insertion losses, ease of fabrication, and integration with other RF circuits in communications systems. The solution proposed in this research work is based on a ceramic substrate with a permittivity of 90, which allowed us to reduce size and make SIW even more attractive. This confirms the feasibility of a SIW solution with a high-permittivity ceramic substrate for the design of filters intended to equip the payload of a satellite. Since C-band is mostly used for satellite and Radar applications. So, proposed SIW filter may be a good candidate to enhance the performance of Satellite application devices.

Futures works will be interesting in SIW for coupled interlinked split ring resonator based epsilon negative metamaterial with high effective medium ratio for multiband satellite and radar communications.

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NOMENCLATURE

Q_{ein}	External quality factors of the resonators at the input
Q_{eout}	External quality factors of the resonators at the output
$M_{i,j}$	Coupling coefficient between the resonators i and j for $i, j = 1, 2, 3, \dots, n$
$m_{i,j}$	So-called normalized coupling coefficient for $i, j = 1, 2, 3, \dots, n$
n	Number of the resonators or the order of the filter
FBW	Designed fractional bandwidth
W_M	Width of the conductor
L_M	Length of the conductor
Q_e	External quality factor
P	Distance between the holes
D	Diameter of the metallic via
W_{SIW}	Width of the SIW cavity
L_{SIW}	Length of the SIW cavity
W_T	Width of the transition
L_T	Length of the transition
f_0	Resonant frequency
$\Delta f_{\pm 90^\circ}$	$\pm 90^\circ$ bandwidth of the SIW cavity
$d_{i,j}$	Iris opening between the resonators i and j for $i, j = 1, 2, 3, \dots, n$
R	Diameter of the circular hole etched on the top of the metal layer
W_{CPW}	Width of the conductor backed coplanar waveguide (CBCPW) transition
L_{CPW}	Length of the conductor backed coplanar waveguide (CBCPW) transition

Greek symbols

ϵ_r	Relative permittivity
$\tan\delta$	Loss tangent of the dielectric
σ	Conductivity of the tissue

НОВИ ДИЗАЈН МИНИЈАТУРНИХ СИВ ФИЛТЕРА НА КЕРАМИЧКОМ СУПСТРАТУ ЗА Ц-ПОЈАС

А. Рхабану, А. Ел Фадл, Н. Цебор, С. Бри

Приказују се нове структуре и методе дизајнирања минијатурних интегрисаних таласоводних пропусних (СИВ) филтера на керамичком супстрату велике пропустљивости за ц-појас. Циљ је био да се изврши процена изводљивости таквих филтера коришћењем ЕМ симулатора. Таласовод интегрисан у супстрат (СИВ) нуди квалитет и добре електричне перформансе у поређењу са другим планарним техникама. Могућности интегрисања и трошкови израде чине га атрактивним. Керамички материјал има електрична својства погодна за дизајн пасивних уређаја. Велика релативна пропусност са малим диелектричним губицима омогућава израду пасивних компонента у минијатурним димензијама, при чему постоји велика стабилност на високим температурама, што представља значајан критеријум код избора филтера дизајнираног за опрему корисног терета код сателита. Дизајнирана су три СИВ филтера на Транс-Тек керамичком супстрату (дебљина – 254 μm , $\epsilon_r = 90$, $\tan\delta = 0,0009$) са прецизним спецификацијама за примену у свемиру. Први филтер је састављен од три СИВ резонатора са директним спајањем, други има три СИВ резонатора са попречним спајањем да би пренос био нула, а трећи има три СИВ резонатора са кружним отворима урезаним на врху металног слоја да би се добио супер-широки појас. Резултати истраживања су приказани, размотрени и упоређени са релевантном литературом. Предложени филтер може да се користи за побољшање перформанси микроталасних уређаја за ц-појас, посебно за сателитску комуникацију.